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Antenna array design with Chebychev polynomials

Prof. Eleftheriades desribed a Chebychev antenna array design method that looks different than the one of the text [1].

Portions of that procedure are like that of the text. For example, if a side lobe level of $20 \log_{10} R$ is desired, a scaling factor

$$x_0 = \cosh\left(\frac{1}{m}\cosh^{-1}R\right),\tag{1.1}$$

is used. Given *N* elements in the array, a Chebychev polynomial of degree m = N - 1 is used. That is

$$T_m(x) = \cos\left(m\cos^{-1}x\right). \tag{1.2}$$

Observe that the roots x'_n of this polynomial lie where

$$m\cos^{-1}x'_n = \frac{\pi}{2} \pm \pi n,$$
 (1.3)

or

$$x'_n = \cos\left(\frac{\pi}{2m}\left(2n\pm1\right)\right),\tag{1.4}$$

The class notes use the negative sign, and number $n = 1, 2, \dots, m$. It is noted that the roots are symmetric with $x'_1 = -x'_m$, which can be seen by direct expansion

$$\begin{aligned} x'_{m-r} &= \cos\left(\frac{\pi}{2m} \left(2(m-r) - 1\right)\right) \\ &= \cos\left(\pi - \frac{\pi}{2m} \left(2r + 1\right)\right) \\ &= -\cos\left(\frac{\pi}{2m} \left(2r + 1\right)\right) \\ &= -\cos\left(\frac{\pi}{2m} \left(2(r+1) - 1\right)\right) \\ &= -x'_{r+1}. \quad \Box \end{aligned}$$
(1.5)

The next step in the procedure is the identification

$$u'_{n} = 2\cos^{-1}\left(\frac{x'_{n}}{x_{0}}\right)$$

$$z_{n} = e^{ju'_{n}}.$$
(1.6)

This has a factor of two that does not appear in the Balanis design method. It seems plausible that this factor of two was introduced so that the roots of the array factor z_n are conjugate pairs. Since $\cos^{-1}(-z) = \pi - \cos^{-1} z$, this choice leads to such conjugate pairs

$$\exp\left(ju'_{m-r}\right) = \exp\left(j2\cos^{-1}\left(\frac{x'_{m-r}}{x_0}\right)\right)$$
$$= \exp\left(j2\cos^{-1}\left(-\frac{x'_{r+1}}{x_0}\right)\right)$$
$$= \exp\left(j2\left(\pi - \cos^{-1}\left(\frac{x'_{r+1}}{x_0}\right)\right)\right)$$
$$= \exp\left(-ju_{r+1}\right).$$
(1.7)

Because of this, the array factor can be written

$$\begin{aligned} AF &= (z - z_1)(z - z_2) \cdots (z - z_{m-1})(z - z_m) \\ &= (z - z_1)(z - z_1^*)(z - z_2)(z - z_2^*) \cdots \\ &= (z^2 - z(z_1 + z_1^*) + 1) (z^2 - z(z_2 + z_2^*) + 1) \cdots \\ &= \left(z^2 - 2z \cos\left(2\cos^{-1}\left(\frac{x_1'}{x_0}\right)\right) + 1\right) \left(z^2 - 2z \cos\left(2\cos^{-1}\left(\frac{x_2'}{x_0}\right)\right) + 1\right) \cdots \end{aligned}$$
(1.8)
$$&= \left(z^2 - 2z \left(2\left(\frac{x_1'}{x_0}\right)^2 - 1\right) + 1\right) \left(z^2 - 2z \left(2\left(\frac{x_2'}{x_0}\right)^2 - 1\right) + 1\right) \cdots \end{aligned}$$

When m is even, there will only be such conjugate pairs of roots. When m is odd, the remainding factor will be

$$z - e^{2j\cos^{-1}(0/x_0)} = z - e^{2j\pi/2} = z - e^{j\pi} = z + 1.$$
(1.9)

Example 1.1: Expand AF for N = 4.

The roots of $T_3(x)$ are

$$x_n' \in \left\{0, \pm \frac{\sqrt{3}}{2}\right\},\tag{1.10}$$

so the array factor is

$$AF = \left(z^2 + z\left(2 - \frac{3}{x_0^2}\right) + 1\right)(z+1)$$

= $z^3 + 3z^2\left(1 - \frac{1}{x_0^2}\right) + 3z\left(1 - \frac{1}{x_0^2}\right) + 1.$ (1.11)

With $20 \log_{10} R = 30$ dB, $x_0 = 2.1$, so this is

$$AF = z^3 + 2.33089z^2 + 2.33089z + 1.$$
(1.12)

With

$$z = e^{j(u+u_0)}$$

$$= e^{jkd\cos\theta + jku_0}.$$
(1.13)

the array factor takes the form

$$AF = e^{j3kd\cos\theta + j3ku_0} + 2.33089e^{j2kd\cos\theta + j2ku_0} + 2.33089e^{jkd\cos\theta + jku_0} + 1.$$
(1.14)

This array function is highly phase dependent, plotted for $u_0 = 0$ in fig. 1.1, and fig. 1.2.



Figure 1.1: Plot with $u_0 = 0$, $d = \lambda/4$.



Figure 1.2: Spherical plot with $u_0 = 0$, $d = \lambda/4$.

This can be directed along a single direction (z-axis) with higher phase choices as illustrated in fig. **1.3**, and fig. **1.4**.



Bibliography

[1] Constantine A Balanis. *Antenna theory: analysis and design*. John Wiley & Sons, 3rd edition, 2005. 1